Europäisches Patentamt
European Patent Office
Office européen des brevets

(19) (11) Publication number: **0 126 626 A2**

(12) **EUROPEAN PATENT APPLICATION**

(21) Application number: **84303356.4**

(22) Date of filing: **17.05.84**

(51) Int. Cl.³: **H 01 Q 3/26**

(30) Priority: **23.05.83 US 497349**
23.05.83 US 497350

(43) Date of publication of application: **28.11.84**
Bulletin 84/48

(84) Designated Contracting States: **DE FR GB IT NL SE**

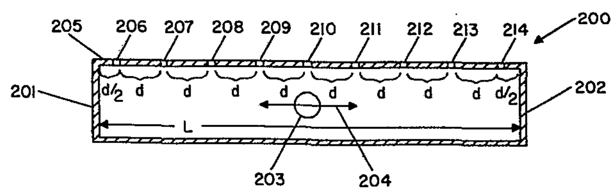
(71) Applicant: **HAZELTINE CORPORATION, 500 Commack Road, Commack New York 11725 (US)**

(72) Inventor: **Frazita, Richard F., 12 Skunks Hollow Road, St. James New York 11780 (US)**
Inventor: **Lopez, Alfred R., 4 Sarina Drive, Commack New York 11725 (US)**

(74) Representative: **Wood, Anthony Charles et al, c/o MICHAEL BURNSIDE & PARTNERS 2 Serjeants' Inn Fleet Street, London EC4Y 1HL (GB)**

(54) **Resonant waveguide aperture manifold.**

(57) A waveguide manifold (200) for monitoring the operation of an array antenna (1). The waveguide is centerfed (203) and has reflecting terminations (201, 202) at either end. The waveguide output is matched to the waveguide as if non-reflecting terminations were at either end of the waveguide. The waveguide input is a plurality of groups of slots (206-214) wherein adjacent slots in each group (A, B, C, D) have alternating polarity and adjacent groups may have alternating phase. A standing wave created in the waveguide has a plurality of cells of alternating phase (Fig. 11). Each slot is located within one of the resonating standing wave cells. The resulting manifold beam forming characteristic will be temperature and frequency independent over a practical range.



EP 0 126 626 A2

Docket R4287/78.07
FRA:mfk

RESONANT WAVEGUIDE APERTURE MANIFOLD

The invention relates generally to phase-stable manifolds and, in particular, a resonant waveguide for monitoring a scanning beam antenna essentially independent of temperature and frequency over a practical range and for monitoring a scanning beam antenna at a scan angle which is not aligned with the boresight direction of the antenna.

Slotted waveguides are sometimes used as aperture manifolds which couple to the radiated signal of a phased-array antenna to monitor its performance. Such waveguide manifolds are used in Microwave Landing System (MLS) ground systems for producing a signal equivalent to a signal viewed by a receiver at a specific angle within the coverage volume of the ground system. Ideally, such waveguide manifolds provide a far-field view of the scanning beam of the ground system and, additionally, measure the antenna insertion phase and amplitude associated with each individual array element.

Waveguide manifolds used to monitor elevation and azimuth scanning beams of an MLS ground system have been waveguides which propagate travelling waves and, consequently, the phasing characteristics are frequency and temperature dependent. The result is that the scan angle of the beam monitored at the waveguide output is also temperature and frequency dependent. Furthermore, for monitoring MLS azimuth scanning, a travelling wave manifold does not inherently monitor the zero degree course over the MLS operating frequency bandwidth. This is because the beam pointing characteristic of a travelling wave manifold is frequency and temperature dependent.

It is an object of this invention to provide a resonant waveguide aperture manifold that forms a beam at a scan angle that is independent of temperature and frequency.

The apparatus according to the invention comprises a transmission line for directing electromagnetic energy in a predetermined frequency range. Associated with the line are elements such as coupling slots or holes. The line may be associated with groups of elements such as coupling slots or holes wherein adjacent groups have different phase. Each group has N elements wherein adjacent elements have different phase, N being a positive integer greater than one.

A transducer is associated with the line for converting energy having a frequency within the predetermined frequency range into an electrical signal having a corresponding frequency and vice versa. The transducer has an impedance which is matched to the line as if the line had non-reflecting terminations coupled to the first and second ends thereof. First means creates a short circuit at the first end of the line and second means creates a short circuit at the second end of the line.

For a better understanding of the present invention, together with other and further objects, reference is made to the following description, taken in conjunction with the accompanying drawings, and its scope will be pointed out in the appended claims.

Figure 1 is a longitudinal cross-sectional view of a travelling waveguide according to the prior art.

Figure 2 is a simplified block diagram illustrating one use of an aperture manifold as described in copending European Application No.83.304471.2 filed 3rd August 1983 for Scanning Antenna With Automatic Beam Stabilization, incorporated herein by reference.

Figure 3 is a longitudinal cross-sectional view of a resonant waveguide according to the invention.

Figure 4A is a perspective view of one side of a resonant waveguide according to the invention showing the slots therein.

Figure 4B is a perspective view of one side of an asymmetric resonant waveguide according to the invention showing the adjacent groups of slots of alternating phase wherein each group has adjacent slots of alternating phase.

Figure 5 is a transverse cross-sectional view of one resonant waveguide according to the invention illustrating its rectangular configuration.

Figure 6 is a transverse cross-sectional view of another resonant waveguide according to the invention illustrating its ridged rectangular configuration.

Figure 7 is an amplitude diagram of an incident wave propagating within a waveguide according to the invention.

Figure 8 is a phase diagram of an incident wave propagating within a waveguide according to the invention.

Figure 9 is an amplitude diagram of a reflected wave propagating within a waveguide according to the invention.

Figure 10 is a phase diagram of a reflected wave propagating within a waveguide according to the invention.

Figure 11 is a diagram of the standing wave generated within a resonant waveguide according to the invention.

Figure 12 is one illustration of the resonant waveguide according to the invention coupled by means of slots to the radiating waveguide column of an MLS azimuth antenna.

Figure 13 is another illustration of a resonant waveguide according to the invention coupled by means of holes to the radiating waveguide column of an MLS azimuth antenna.

Figure 14 is an illustration of a resonant waveguide according to the invention coupled by means of slots to the radiating waveguide column of an MLS elevation antenna.

As shown in figure 1, a prior art travelling wave manifold 100 made of conductive material is provided with an output transducer such as connector 101 which receives a wave propagating along propagation path 102 which is terminated in absorber 103 or other non-reflecting terminating means at the far end. Side 104 functions as a short circuit which reflects waves propagating to the left. Side 105 of waveguide 100 is provided with weakly coupled input slots 106, 107, 108, 109, 110, 111, 112 and 113 having spacing d. The phase relationship between adjacent slots 106 and 107 is given by the following formula:

$$\phi_{107} = \phi_{106} + \frac{2\pi}{\lambda_g} d \pm \pi$$

As shown by the formula, the phase of slot 107 (ϕ_{107}) as compared to the phase of slot 106 (ϕ_{106}) is dependent upon the spacing d and the waveguide wavelength (λ_g). All other adjacent slots have similar phase relationships. Since spacing d is temperature dependent (conductive material such as copper or aluminum expands or contracts with temperature variations) and the waveguide wavelength λ_g is frequency dependent, travelling wave manifold 100 is both frequency and temperature dependent.

The monitored beam pointing angle, 0, for the travelling wave manifold having slots of alternating phase is defined as the pointing angle of a beam provided at the manifold output connector as a result of excitations imparted at the manifold slots. By reciprocity, it may be defined as the conjugate of the pointing angle of a beam radiated by the manifold output slots as a result of excitations imparted by the manifold input connector. The monitored beam pointing angle is given by:

$$\theta = \text{arc sin} \sqrt{(1 - (\lambda_o f_o/\lambda_{co} f)^2 - \lambda_o f_o/2df)}$$

where

λ_o = reference free space wavelength (design center)

λ_{co} = waveguide cutoff wavelength

f_o = reference frequency

f = frequency of excitations

This equation gives the explicit relationship between the monitored beam pointing angle, frequency and coupling slot spacing. The invention relates to: (a) microwave landing systems which use wide scanning phased array antenna systems having a sharp cutoff of the element pattern, such as are disclosed by Richard F. Frazita, Alfred R. Lopez and Richard J. Giannini in U.S. Patent No. 4,041,501; and (b) calibration of a system having plural signal carrying channels.

Referring to Figure 2, generally such antenna systems include one or more radiating elements forming an array 1 in which the elements are arranged along an array axis and are spaced from each other by a given distance. Each of the elements is coupled to a power divider 8 via a corresponding one of a plurality of phase shifters 9 connected to the elements by distribution network 2. Wave energy signals from signal generator 11 and power divider 8 are supplied to antenna elements 1 by phase shifters 9 such that a proper selection of the relative phase values for phase shifters 9 causes antenna elements 12 to radiate a desired radiation pattern into a selected angular region of space. Variation of the relative phase values of the phase shifters 9 is accomplished by beam steering unit 10 via control line 22 and causes the radiated antenna pattern to change direction with respect to angle A in space. Therefore, phase shifters 9 and beam steering unit 10 together form means 2 for scanning a beam radiated by the antenna elements of array 1 as a result of the supplied wave energy signals from generator 11 coupled to the elements of array 1 by power divider 8 and distribution network 2.

The properties of a scanning antenna and techniques for selecting design parameters such as aperture length, element spacing and the particular configuration of the distribution network 2 are well known in the prior art. A review of these parameters is completely described in U.S. Patent No. 4,041,501.

In order to stabilize the beam pointing angle of the radiated beam, an aperture manifold 4 is associated with the antenna elements of array 1. Manifold 4 may be any means for forming a signal provided by output 12 which represents a beam pointing angle of the radiated beam. Preferably, manifold 4 is a highly phase stable waveguide or manifold, such as the invention, coupled to the array 2 and center-fed to avoid inherent frequency (phase) and temperature effects. Center feeding also eliminates first-order dependence on frequency and absolute temperature variations.

As used herein, manifold 4 refers to any type of device for sampling signals including a waveguide, a printed circuit network, a coaxial line network or a power combiner. A phase stable manifold is, by definition, one in which the beam formed by summing of the slot excitations is insensitive to frequency and temperature changes and is used in combination with a phased arrray in accordance with this invention to detect bias error at a specific angle. Manifold 4 is equivalent in function to a probe located in space at a specific angle with respect to the phased array. A manifold in accordance with the present invention may be a slotted waveguide configured to monitor radiated energy such that there is equal, non-zero phase and equal amplitude at all sample points (i.e. slot locations) of the manifold.

The output 12 of manifold 4 is coupled to means 5, associated with means 3, for controlling the scanning of the radiated beam in response to the output 12 of manifold 4.

Figure 3 illustrates a resonant waveguide 200 according to the invention. Waveguide 200 is provided with a first end 201 terminating in a short circuit such as a conductive sheet of metal perpendicular to the sides of waveguide 200 and a second end 202 terminating in a short circuit. Waveguide 200 is center fed by a transducer which converts an electrical signal into electromagnetic energy and vice versa. Preferably, the transducer is any connector well known in the prior art such as output connector 203 which receive waves propagating in both directions along path 204. Side 205 of waveguide 200 is provided with slots 206, 207, 208, 209, 210, 211, 212, 213, and 214 for coupling to a radiating antenna. Figure 4 illustrates a 180^{o} degree phase compensating pattern of the coupling slots which will be described below. Figures 5 and 6 illustrate preferred rectangular crossections of waveguide 200.

As shown by Figure 7, an incident wave radiated by connector 203 has a constant amplitude A_{inc} along the entire length of waveguide 200. This is because amplitude tapers in the travelling wave caused by the coupling slots is counteracted and eliminated by the resonance of waveguide 200.

Due to reciprocity, waveguide 200 may be used in either a transmitting or receiving mode. In the transmitting mode, connector 203 is connected via isolator 215 to a signal source (not shown). The signal is converted by connector 203 to electromagnetic wave energy which propagates along waveguide 200 and is radiated by slots 206-214. In the receiving mode, slots 206-214 are illuminated by electromagnetic wave energy which propagates along waveguide 200 and is converted by connector 203 into an electrical signal. For convenience and according to convention, the invention has been described in a receiving mode. However, this disclosure and the scope of the claims appended hereto should not be limited to any one mode and should be broadly construed to include both transmitting and/or receiving operations.

Figure 8 is an illustration of the incident phase $\emptyset_{inc}$ of the wave radiated by connector 203 and illustrates that the phase along waveguide 200 is linearly changing.

Since short circuits 201 and 202 reflect the incident waves propagating within waveguide 200, figure 9 illustrates that the amplitude of the reflected wave A_{ref} is constant along the entire length of waveguide 200. Similarly, the phase of the reflected wave $\emptyset_{ref}$ propagating within waveguide 200 is linearly changing with distance. The result, as illustrated in figure 11, is a standing wave having a plurality of cells of alternating phase of zero degrees and 180 degrees between spacing d of the slots.

As shown in Figure 4A, each slot is located within one of the standing wave cells of waveguide 200 so that the resulting manifold output will be temperature and frequency independent as long as the variations in temperature and frequency are within the range such that there is one and only one slot or group of slots located within each standing wave cell. By alternating the direction and thereby the phase of adjacent slots, the resulting manifold output will provide equal phasing to all radiating elements. This aperture manifold provides a beam forming capability which is independent of frequency and temperature since the phase within each standing wave cell is constant. To prevent transmission of the reflected wave back through connector 203, isolator 215 is located within the line feeding connector 203.

As shown in Figure 4B, each slot is located within one of the standing wave cells of waveguide 200. By alternating the direction and thereby the phase of the slots, the resulting manifold output will have equal phase for each coupling slot and will be temperature and frequency independent as long as the variations in temperature and frequency are within the range such that there is one and only one slot or group of slots located within each standing wave cell. By alternating the direction and thereby the phase of each group A, B, C and D of slots (N=2) and by alternating direction and thereby the phase of adjacent slots within each group, the resulting manifold output will approximate an 11.25° beam pointing angle. This aperture manifold provides a beam forming capability which is independent of frequency and temperature since the phase within each standing wave cell is constant. To prevent transmission of the reflected wave back through connector 203, isolator 215 is located within the line feeding connector 203.

The monitored beam pointing angle, θ, for resonant manifold 200 according to the invention, over the operational frequency bandwidth, is given by:

$$\theta = \arcsin \frac{0.5}{md/\lambda g}, \quad m = 1, 2 \ldots \infty$$

where $d/\lambda g$ is the slot spacing in guide wavelengths. Therefore, the phasing of manifold 200 is independent of frequency and coupling slot spacing over the operational frequency bandwidth. In the embodiment illustrated in Figure 4A, $\theta = 0^{\circ}$ ($m = \infty$) and the beam radiated is perpendicular to path 204. In the embodiment illustrated in Figure 4B, the beam pointing angle is generally not 0° and the beam radiated by manifold 200 is not perpendicular to path 204 because of the nonequal phasing of the groups of slots. For example, an MLS ground system having a center operating frequency of 5.06GHz (i.e. λ = 2.33 inches) and a group spacing (dg) of 5.97" would have a monitored beam pointing angle of 11.25^{0}.

However, slots 206-214 may be phased to approximate any beam pointing angle desired. The range of the actual beam pointing angles which the slots of a particular manifold may approximate are limited by the physical configuration of the particular manifold. In any case, therefore, the phasing of manifold 200 is independent of frequency and coupling slot spacing over the operational frequency bandwidth.

In order to achieve the results described above, input connector 205 is initially matched to waveguide 200 as if each end of waveguide 200 terminated in a non-reflecting absorber as shown in the prior art illustrated in figure 1. Such a matched connector 205 is employed with waveguide 200 terminating in short circuits as illustrated in figure 2 thereby resulting in the resonant standing wave as shown in figure 9.

To achieve the in-phase condition of the adjacent coupling slots of waveguide 200, the required waveguide wavelength λg is twice the spacing d between coupling slots 206-214. This spacing d is determined by the radiating characteristics of the phased array antenna associated with waveguide 200 and is typically slightly larger than 1/2 wavelength. For the Microwave Landing System elevation phased array antenna, ridge loading as shown in Figure 6 is used to obtain this result. In particular, opposing ridges 250R and 260R are located within waveguide 200R for eliminating odd mode resonance which may disturb the amplitude and phase of the slot excitations.

The maximum length, L, of a manifold according to the invention is limited by the operational frequency bandwidth of the phased array antenna with which it is associated. To limit the beam distortions caused by amplitude taper at the band edges, length L should not exceed the value given below:

$$L \leq \lambda_o f_o / 2\left(f_{max}\sqrt{(1 - (1 - \lambda_o f_o/\lambda_{co} f_{max})^2)} - f_{min}\sqrt{(1 - (1 - \lambda_o f_o/\lambda_{co} f_{min})^2)}\right)$$

For the ICAO standard Microwave Landing System bandwidth, L is given approximately by:

$$L \approx \frac{\lambda_g f_o}{2\Delta f}$$

where $\Delta f/fo$ is the fractional design bandwidth plus a margin for fabrication tolerances.

For $\Delta f/fo = .0165$, $L = 30.3\ \lambda g$. For larger arrays on the order of 60 λ_g, two similar manifolds can be interconnected with equal length stable transmission lines.

Figure 12 illustrates waveguide 200R in association with waveguide 300 such as descibed by U.S. Patent No. 3,903,524, owned by Hazeltine Corporation. Waveguide 300 may be one of a series of parallel waveguides forming the azimuth antenna of a Microwave Landing System (MLS) ground system. Such a ground system requires monitoring to evaluate its performance. In order to provide such monitoring, waveguide 200R functions as a manifold and is associated with each of the parallel waveguides 300. Ridge loading in waveguide 200R in the form of ridges 250R and 260R is used to match the guide wavelength of waveguide 200 to the required spacing of radiating waveguides 300. Specifically, waveguide 300 with polarized radiating slots 301 has a non-polarized opening 302 coupled to slot 208R. Other vertical waveguides would be coupled to slots 206R and 207R.

Figure 13 illustrates another MLS ground system coupling configuration having non-polarized holes 506R, 507R and 508R in broad wall 509R of waveguide 500R and having ridge 510R on broad wall 511R. The non-polarized holes are coupled to parallel radiating waveguides such as waveguide 300 by polarized slot 303. For this configuration the required 180 degree phase reversals between adjacent coupling holes is incorporated in the design of waveguide 300. Adjacent waveguides 300 have a 180^0 phase reversal at their input wave launchers i.e. slot 303.

Figure 14 illustrates another MLS ground system coupling configuration wherein slots 206, 206a, 207, 207a, 208, 208a, are coupled to dipole array 400 which may function as an MLS elevation antenna. Although this invention has been particularly described with regard to its function as an elevation manifold, it may be used as an azimuth manifold or other array monitor.

CLAIMS

1. Apparatus comprising a transmission line (200) for directing electromagnetic energy in a predetermined frequency range, said line having first and second ends; and elements (206-214) associated with said line; said apparatus characterised by:

(a) a transducer (203) associated with said line for converting energy having a frequency within the predetermined frequency range into an electrical signal having a corresponding frequency and vice versa, said transducer having an impedance which is matched to said line as if said line had substantially non-reflecting terminations coupled to the first and second ends thereof;

(b) a first short circuit (201) at the first end of said line; and

(c) a second short circuit (202) at the second end of said line.

2. Apparatus according to claim 1 wherein adjacent elements (Fig. 4A) have different phases.

3. Apparatus according to claim 1 or claim 2 wherein said transmission line (200) comprises an electrically conductive hollow member and said elements comprise openings (206-214, 506-508) in said member.

4. Apparatus according to claim 3 wherein said electrically conductive hollow member is a linear waveguide of rectangular cross-section (Figures 5

and 6) and said openings comprise a linear array of slots spaced apart by substantially one-half of the waveguide wavelength of said member (Figure 3).

5. Apparatus according to claim 4 wherein said transducer comprises a connector (203) projecting into said member.

6. Apparatus according to claim 5 further including a circuit (215) for isolating from the waveguide any load connected to the connector.

7. Apparatus acording to any one of claims 4 to 6 wherein said first short circuit (201) comprises a first electrically conductive member substantially perpendicular to the sides of said waveguide and attached to the first end, and said second short circuit comprises a second electrically conductive member substantially perpendicular to the sides of said waveguide and attached to the second end (Figure 3).

8. Apparatus according to any one of claims 1 to 7 wherein adjacent elements have opposite phases (Figure 4A).

9. Apparatus according to any one of claims 1 to 8 further including apparatus (250,260) for eliminating odd mode resonance thereby reducing amplitude and phase distortions of the element excitations.

10. Apparatus according to claim 9 wherein said apparatus for eliminating comprises a ridge (250, 260) located within said member.

11. Apparatus according to any one of claims 1 to 10 comprising: groups (A,B,C, D) of elements associated with said line wherein adjacent groups have different phase (Figure 4B), each group having N elements wherein adjacent elements within each group have different phases, where N is a positive even integer greater than one; whereby supplying an electrical signal having a frequency within the predetermined frequency range to the transducer results in the elements radiating a beam which is not perpendicular to the transmission line.

12. Apparatus according to claim 11 wherein said elements are waveguide slots configured to approximate a beam pointing angle of approximately 11.25^{0}(Figure 4B).

13. Apparatus according to claim 11 or claim 12 wherein adjacent groups (AB,BC,CD) of elements have opposite phases and adjacent elements within each group have opposite phases (Figure 4B).

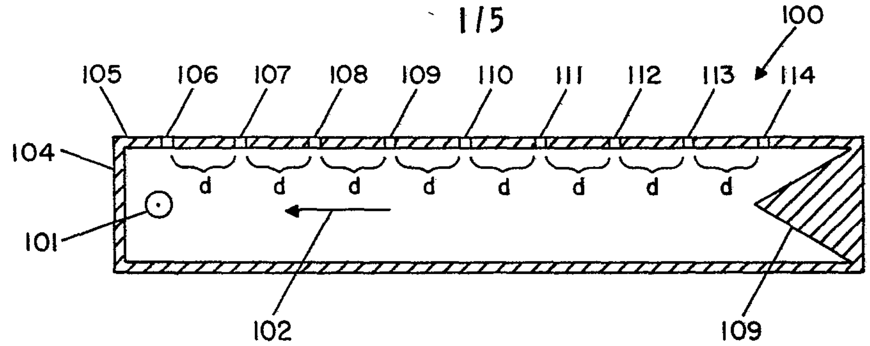


FIG. 1 PRIOR ART

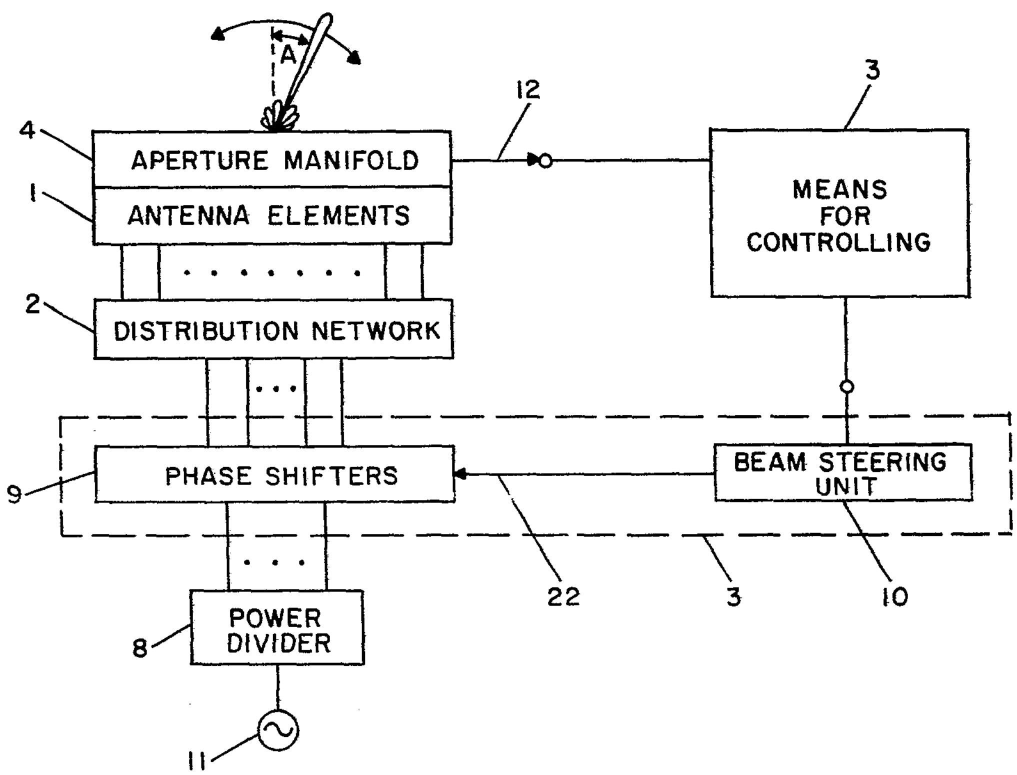


FIG. 2

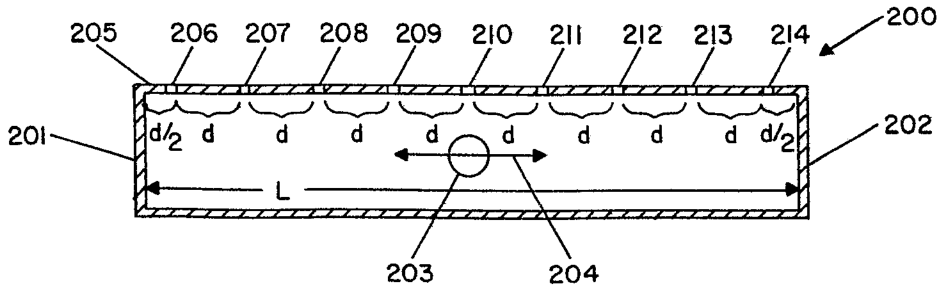


FIG. 3

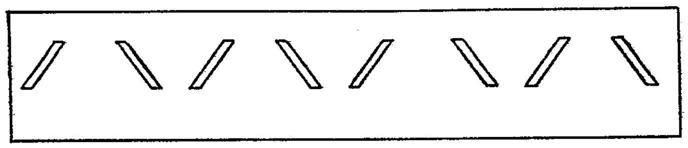


FIG. 4A

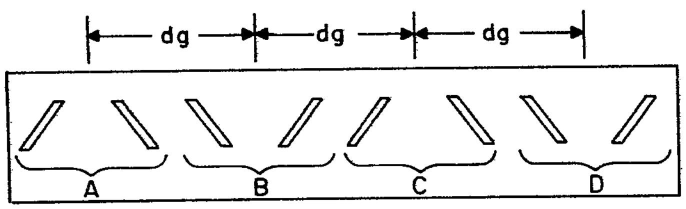


FIG. 4B

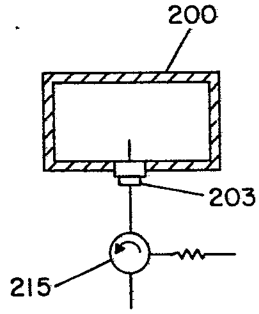


FIG. 5

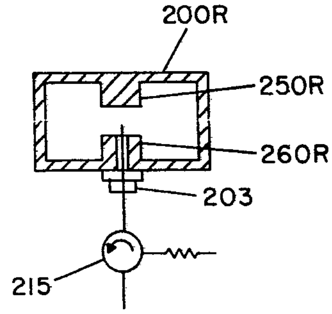


FIG. 6

FIG. 7

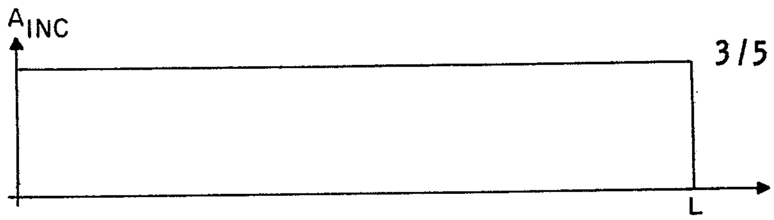


FIG. 8

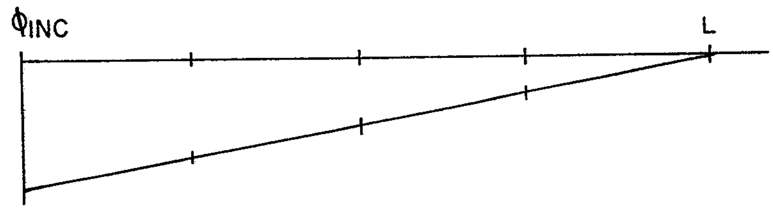


FIG. 9

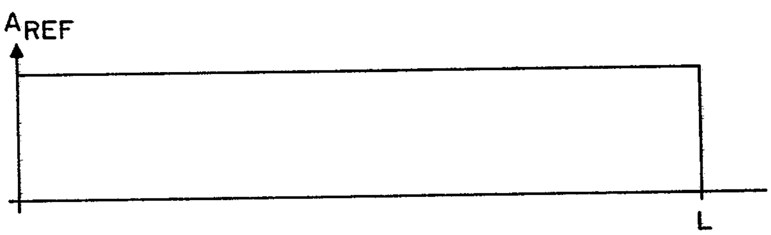


FIG. 10

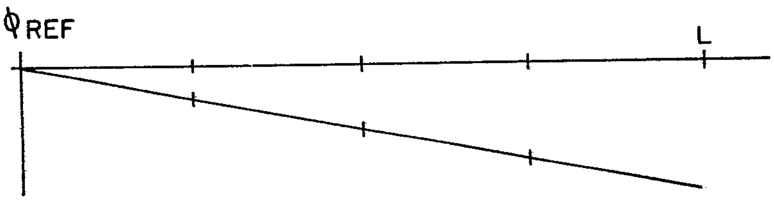
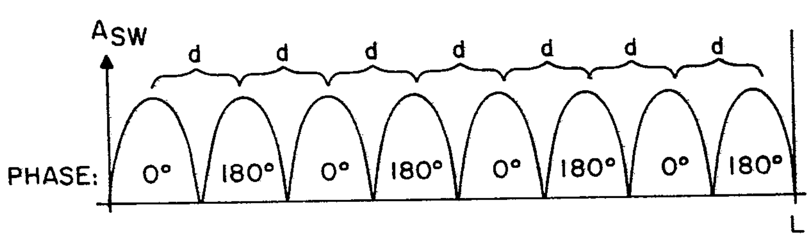


FIG. 11



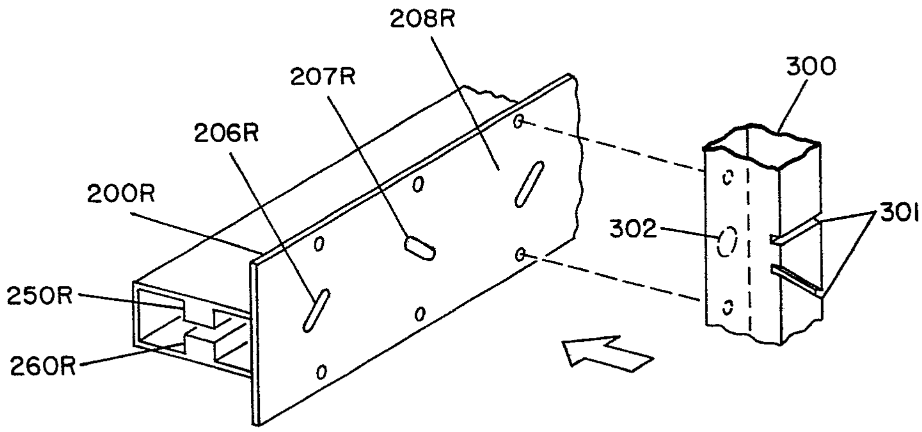

208R
207R
206R
200R
250R
260R
300
301
302

FIG. 12

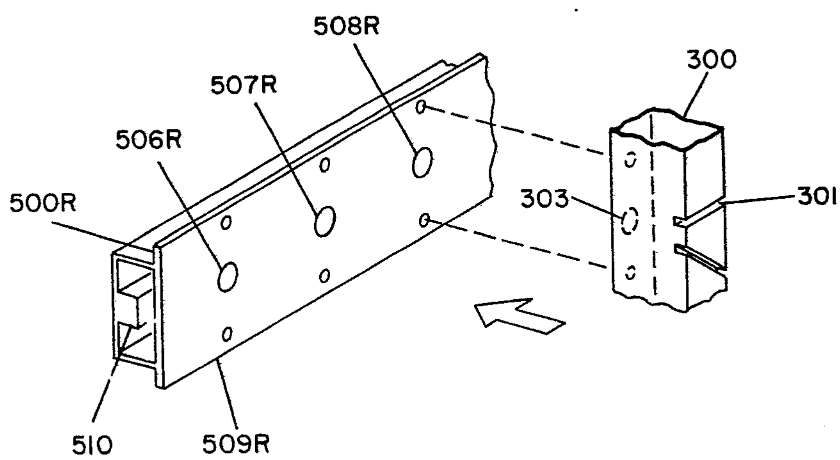

508R
507R
506R
500R
510
509R
300
303
301

FIG. 13

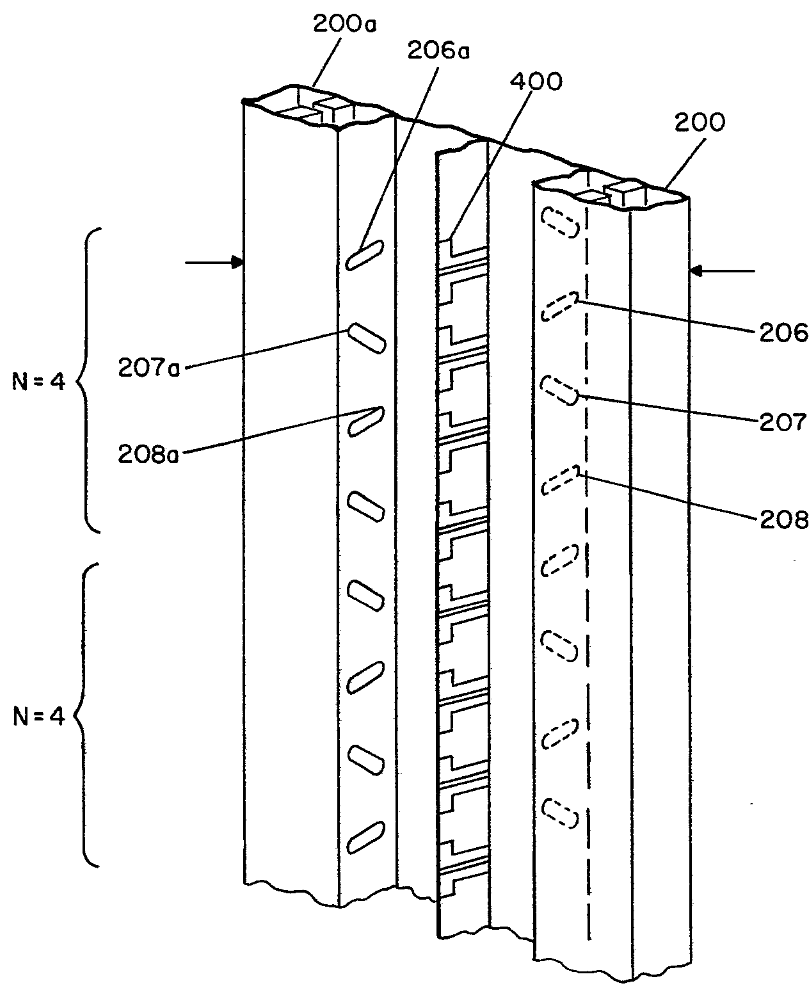


FIG. 14